Abstract—Three-phase voltage-source converters are used as utility interfaces. In such a case, the converter line currents are required to track sinusoidal references synchronized with the utility grid without a steady-state error. In this paper a current control method based on a sinusoidal internal model is employed. The method uses a sine transfer function with a specified resonant frequency, which is called an S regulator. The combination of a conventional proportional–integral (PI) regulator and an S regulator is called a PIS regulator. The PIS regulator ensures that the steady-state error in response to any step changes in a reference signal at the resonant frequency and 0 Hz reduces to zero. An experiment was carried out using a 1-kVA prototype of three utility-interface converters, a voltage-source rectifier, an active power filter, and static synchronous compensator. Almost perfect current-tracking performance could be observed.

Index Terms—Active filter, sinusoidal internal model, static synchronous compensator (STATCOM), voltage-source pulsewidth-modulation (PWM) converter.

I. INTRODUCTION

DEVELOPMENT of renewable and clean energy sources such as photovoltaic, wind, and fuel cells, is growing. Since the majority of such sources generate a dc voltage, a voltage-source pulsewidth-modulation (PWM) inverter and its control technique are essential to connect them to the utility grid [1].

The focus on power quality has been increased with the increased use of power electronic equipment. Harmonic current and reactive current are two of the parameters that characterize the power quality. An active filter and a static synchronous compensator (STATCOM) are expected to be candidates to improve the power quality [2].

In those cases, a three-phase voltage-source PWM inverter/rectifier plays an important role as a power electronic interface to the utility grid. The ac current of the converter is required to be harmonic free and to track rapidly a sinusoidal reference without a steady-state error. In this situation, the following three current-regulating techniques have been used [3], [4]:


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1) hysteresis control;
2) predictive control;
3) ramp comparison.

Hysteresis control has the attraction of simplicity, but leads to a widely varying switching frequency. This limitation has been improved with variable hysteresis band switching strategies but it requires a complex controller to achieve satisfactory performance [5]. Predictive current control offers the best potential for precise current control, but implementation of a practical system can be difficult and complex [6].

Ramp comparison control using a proportional-integral (PI) regulator has a long history of use, but has the disadvantage of a steady-state error between the reference current and the output current if the reference is a sinusoidal signal. This drawback can be solved if the current control is executed in a synchronous d–q coordinate reference frame [3]. A synchronous d–q reference frame is appropriate since the steady-state currents are dc currents and a simple PI regulator will result in zero steady-state error. However, it is more complex and requires more hardware or software for implementation because of the requirement to transfer the measured currents to a synchronous frame and, subsequently, transform the output of the PI regulator back to a stationary frame to drive the ramp comparison controller.

In contrast to the synchronous reference frame control, stationary reference frame control based on the internal model principle from control theory was proposed and was applied to a single-phase active filter [7]. In this paper, a sinusoidal internal model is employed to control a three-phase voltage-source PWM converter for three different utility-interface applications:

- active power filter (AF);
- PWM voltage-source boost rectifier (VSR);
- static synchronous compensator (STATCOM).

The sinusoidal internal model requires a transfer function of a sine wave in the regulator, and it is called an S regulator. In this paper, the validity of an S regulator for the control of utility interface converters is demonstrated by experimental results. No coordinate transformation is required and no steady-state error remains if a PI and S regulator is used.

II. PIS REGULATOR

Consider feedback control of a PWM inverter output current. If \( G_{\text{inv}}(s) \), \( G_{\text{load}}(s) \), and \( G_C(s) \) represent the transfer functions of the PWM inverter, load, and current regulator,
respectively, the inverter output current \( i_C \) with \( i_{C^*} \) being a current reference will be given by

\[
\dot{i}_C = \frac{G_C G_{\text{inv}} G_{\text{load}}}{1 + G_C G_{\text{inv}} G_{\text{load}}} i^*_{C^*}
\]

A PI and S regulator is defined as a regulator consisting of a proportional (P) action, an integral (I) action, and a transfer function of a sine wave (S action), and is, hereafter, called a PIS regulator.

The transfer function of the PIS regulator will be given by

\[
G_C(s) = K_p + \frac{K_i}{s} + \frac{K_\alpha s}{s^2 + \omega_0^2}
\]

where \( \omega_0 \) denotes the resonant frequency of the sine transfer function, and \( K_p, K_i, \) and \( K_\alpha \) represent the respective gains. The resonant frequency \( \omega_0 \) is designed to coincide with the frequency of a sinusoidal reference input \( i^*_{C^*} \). If the PIS regulator is used, (1) indicates that the gain of the open-loop transfer function, \( G_C(s)G_{\text{inv}}(s)G_{\text{load}}(s) \), increases to infinity at the frequency \( \omega_0 \) and 0 Hz. This ensures that the steady-state error \( \dot{i}_C^* - i_C \) in response to a step command change at those frequencies will reduce to zero as far as the system is stable. Furthermore, the PIS regulator will remove the effect of a disturbance at those frequencies. Experimental results in the following three sections demonstrate the usefulness of the PIS regulator.

If the reference \( i^*_{C^*} \) does not include a dc component as the case of a utility interface converters, an integral regulator may be omitted, and a PIS regulator degenerates to a PS regulator.

A. Design of PS Regulator

The open loop transfer function of an inverter output current control system with an \( L-R \) load will be given by

\[
G(s) = \left( K_p + \frac{K_\alpha s}{s^2 + \omega_0^2} \right) G_{\text{inv}}(s) \frac{1}{R + Ls}.
\]

The Bode diagram of (3) with only a P regulator \( (K_i = 0) \) and with a PS regulator are compared in Fig. 1, where the transfer function of the inverter is assumed to be unity, \( G_{\text{inv}}(s) = 1 \). The load consists of \( R = 8.8 \Omega \) and \( L = 49.5 \text{ mH} \), and the resonant frequency is \( \omega_0 = 100 \text{ rad/s} \). The gains are \( K_p = 100 \text{ V/A} \) and \( K_\alpha = 10 \text{ 000 V/A-s} \). One can observe that the influence of the S regulator is confined to the area near the resonant frequency and, thus, the P regulator determines major dynamic characteristics. Accordingly, the dynamic performance of the inverter will be governed by the P regulator gain \( K_p \).

PS regulators exhibit excellent control performance for a sinusoidal reference, but there is no general rule to design their respective gains such as Ziegler–Nichols rules for PI regulators. Thus, the gain design is based on the rule of trial and error.

The following is a manner to design the gains that the authors obtained empirically through their experiment. The P gain is determined first, and the S gain is determined last.

1) Find the range of the proportional gain \( K_p \) with which the phase margin and gain margin of (3) are between 40°–60° and 10–20 dB, respectively [8], considering a stable and rapid response.

2) Conduct an experiment on responses to a step change in the current reference using several different \( K_p \)’s within the range obtained at the first step. The authors recommend that the currents are transformed to a synchronous \( d-q \) reference frame, which allows one an easier evaluation of the responses because the steady-state currents are dc currents.

3) Such experimental investigation indicates that if \( K_p \) is small the responses are slow as shown in Fig. 2(a). If \( K_p \) is too large the responses are rapid but the control reacts to noises as shown in Fig. 2(b). Thus, the authors select the largest \( K_p \) with which the control does not react to noises.

4) Conduct an experiment on responses to a step change in the reference current using the selected \( K_p \). If \( K_\alpha \) is small the responses are slow as shown in Fig. 2(c), and if \( K_\alpha \) is too large the responses are rapid but the output overshoots the reference as shown in Fig. 2(d). The authors select the largest \( K_\alpha \) with which the output does not overshoot the reference. The step responses with the selected gains are shown in Fig. 2(e).

The gains selected in this manner have an approximate relation \( K_\alpha = 100K_p \). This relation is not general, but held even in the three different utility-interface applications described later, VSR, AF, and STATCOM with a sampling frequency of 10 kHz. This fact is helpful in designing the best gain values of PS regulators.

If experiment-based examinations described above are not possible, simulation-based examinations according to the same steps mentioned above are also useful. From the authors’ experience, simulation-based examinations provide fairly close gain values to optimal ones, but it should be noted that in most cases they provide optimistic results, that is, larger gains than optimal which the experimental examinations provide.
Fig. 2. Comparison of step responses with different PS gains, $K_p$ and $K_s$. (a) $K_p = 10$ V/A, and $K_s = 10,000$ V/A/s. (b) $K_p = 400$ V/A, and $K_s = 10,000$ V/A/s. (c) $K_p = 100$ V/A, and $K_s = 5,000$ V/A/s. (d) $K_p = 100$ V/A, and $K_s = 20,000$ V/A/s. (e) $K_p = 100$ V/A, and $K_s = 10,000$ V/A/s.
Active component currents, which are measured and is kept constant, control; A PI regulator produces a dc current and phase Hz), the error is 1.7% with and which have unity amplitude and are in phase with and of the S regulator constant. V/A are, but is 0.35% with by the normalized voltage signals of the S regulator be adjusted s. Fig. 3 indicates that a larger. Each were V/A, and respectively. The current control is executed from 50 Hz is 2% (Δf = 1 Hz), the error is 1.7% with K_s = 10 000 V/A-s, but is 0.35% with K_s = 50 000 V/A-s. Since a practical frequency deviation of the utility grid would be less than 0.5% in Japan, it is no problem to keep the resonant frequency ω_0 of the S regulator constant.

B. Robustness of Current Control Using PS Regulator

The utility grid always has a slight frequency deviation. Should the resonant frequency ω_0 of the S regulator be adjusted so as to follow that slight deviation? To answer this question, the examination is made on the robustness of a sinusoidal internal model in terms of frequencies.

The gain diagram near the resonant frequency in Fig. 1 is enlarged, and shown in Fig. 3 together with the gain diagram with K_s = 50 000 V/A-s. Fig. 3 indicates that a larger K_s results in a higher open-loop gain around the resonant frequency. Therefore, it is expected that a slight deviation in the utility frequency would not deteriorate the control performance if large K_s were selected. To confirm this fact, simulation was carried out using the current control system in (3), where the current reference was 5 A, and the reference frequency was varied from 40 to 60 Hz, while the resonant frequency of the S regulator and P gain were kept at f_0 = 50 Hz (ω_0 = 2πf_0) and K_p = 100 V/A, respectively.

Fig. 4 shows the error versus reference frequency characteristic. One can observe the robustness in terms of frequency deviations if large K_s is selected. For example, if the deviation from 50 Hz is 2% (Δf = 1 Hz), the error is 1.7% with K_s = 10 000 V/A-s, but is 0.35% with K_s = 50 000 V/A-s. Since a practical frequency deviation of the utility grid would be less than 0.5% in Japan, it is no problem to keep the resonant frequency ω_0 of the S regulator constant.

Fig. 5 shows the three-phase AF and load system. The control system used for the experiment is also shown in the figure. There are two control criteria:

1) dc voltage, V_{dc}, control;
2) three-phase output currents, i_{uw}, i_{uv}, i_{uw}, control.

In the dc voltage control, V_{dc} is measured and is kept constant at its reference V_{dc}. A PI regulator produces a dc current reference I^*. Active component currents i_{dca} and i_{dwa}, which are required by the AF to compensate for its power losses, are obtained by multiplying I^* by the normalized voltage signals u_{a} and u_{w} which have unity amplitude and are in phase with the supply voltages e_{a} and e_{w}, respectively.

In the current control, the load currents i_{hu} and i_{hw} are measured, and their harmonic components i_{hul} and i_{hwl} are extracted. Current references of the AF are composed of i_{hul} = i_{dca} and i_{hwl} = i_{dwa}, respectively. The current control is executed using two PS regulators installed in phase u and phase w. Each PS regulator includes seven S regulators having different resonant frequencies. Each of the resonant frequencies is tuned to the fundamental, 5th, 7th, 11th, 13th, 17th, and 19th harmonics.

There are two kind diode rectifiers that act as a typical harmonic-producing load in the ac power lines:

1) choke-input rectifiers;
2) capacitor-input rectifiers.

Fig. 5 shows the AF with a choke-input rectifier, and Fig. 6 is the experimental current waveforms when the AF is operating.
The total harmonic distortion (THD) value of the load current $i_{LH}$ was 16.4%, but the AF improved that of the supply current $i_{SH}$ as low as 2.0%. The parameters are listed in Table I.

Fig. 7 shows the current responses when the AF started operation at $t = 82.6$ ms. One can observe that the transient disappeared almost in a half cycle (10 ms) of the supply frequency.

IV. THREE-PHASE VSR

A three-phase VSR is used as a utility interface of renewable energy sources and a front-end converter of adjustable-speed ac drives. A VSR is obtained if the diode rectifier in Fig. 5 is
removed, and a dc load consisting of $R_L$ and $L_L$ is connected across the capacitor $C_d$. There are two control criteria:

1) dc voltage control;
2) three-phase current control.

The dc voltage control is the same as the AF described in Section III. The current control is similar to AF. VSR should draw sinusoidal currents with unity displacement power factor from the ac supply. Thus, an inverted form of the active currents, $i_{di}$ and $i_{dq}$, provides current references. The two PS regulators are installed in phase-$u$ and phase-$w$ to execute the current control. The parameters are listed in Table I.

Experimental waveforms without and with the S regulator are compared in Fig. 10(a) and (b), respectively. When only P regulators were used one can observe that the current waveforms were sinusoidal, but a considerable current error remained. This is because the reference signal is time varying. In contrast, when the PS regulators were used one can observe that the current error was kept at 0 A.

V. THREE-PHASE STATCOM

The circuit and control system of a STATCOM are quite similar to an AF. In a STATCOM, a three-phase ac load consisting of $R_L$ and $L_L$ connected in series replaces the diode rectifier in Fig. 5. The voltage control is the same as the AF described in Section III. The parameters are listed in Table I.

In the current control, the load currents in phase-$u$ and phase-$w$ are measured and their reactive components are extracted. The current references are an inverted form of the reactive component of the respective load currents. Two PS regulators execute this current control.

Fig. 11 shows the voltage and current waveforms when the STATCOM was in operation. As the load was inductive, the load current lagged behind the supply voltage. When the STATCOM was not in operation the supply current and load current were the same, and were 3.75 A in rms. When the STATCOM was operated, it generated a current of 2.8 A to compensate for the reactive component of the load current. Thus, the supply current was reduced down to 2.8 A. One can observe that the supply current is in phase with the supply voltage, which ensures that the displacement power factor of the supply current was at unity.

Fig. 12 shows transient responses when the STATCOM started operation at $t = 464$ ms. In order to clearly distinguish an active component from a reactive component, the three-phase currents are intentionally represented in the synchronous $d-q$ coordinate reference frame.

The currents $i_d$ and $i_q$ correspond to an active and reactive component in the synchronous reference frame, respectively. One can observe that the reactive component in the supply current disappeared in one cycle (20 ms).

VI. CONCLUSION

This paper has proposed the application of a PIS regulator to the current control of utility-interface converters. A PIS regulator does not require any coordinate transformations, but it can
track an arbitrary number of harmonic component, dc, and fundamental frequency reference signals with a zero steady-state error.

Since the line-side currents of utility-interface converters are required to track sinusoidal references synchronized with the utility grid, a PIS regulator is essentially suitable for their current control.

Three applications, a three-phase AF, a VSR, and a STATCOM, have been presented. The advantage of the PIS regulator has been verified by experimental results.

A set of sine transfer functions that results in almost the perfect tracking of harmonic components has been verified using the AF application. It is confirmed using the VSR that the steady-state error for a sinusoidal current reference has been zero. A sine transfer function that results in almost perfect compensation for a reactive component of load current has been verified using the STATCOM application.

Also, this paper has proposed a practical method for deciding gains of a P regulator and an S regulator, which the authors obtained empirically through their experiment.

**REFERENCES**


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